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(54) **METHOD AND APPARATUS FOR REDUCING SPREAD SPECTRUM NOISE**

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(51) **Int. Cl.**⁷ **H04B 1/707**

(52) **U.S. Cl.** **375/148; 375/144**

(58) **Field of Search** **375/130, 140, 375/144, 147, 148; 367/320, 335, 342**

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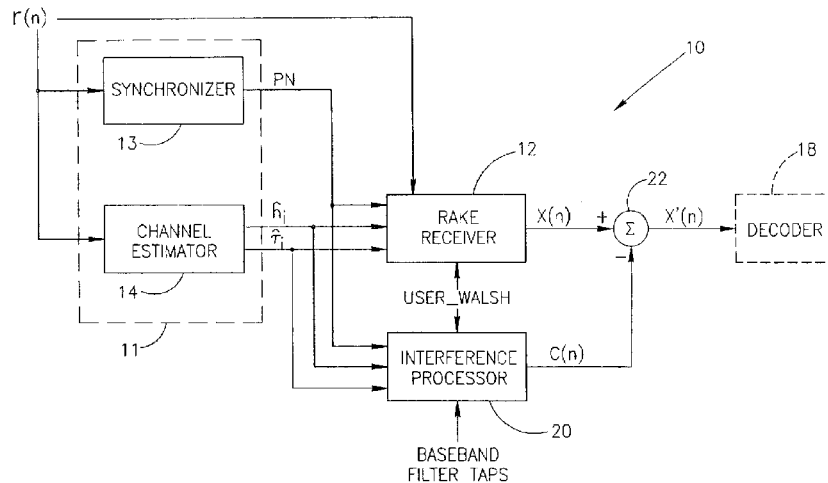
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(57) **ABSTRACT**

A communication device including a per finger interference reducer adapted to remove an interference effect of at least one pilot signal from the output of a despreader of the finger.

12 Claims, 7 Drawing Sheets



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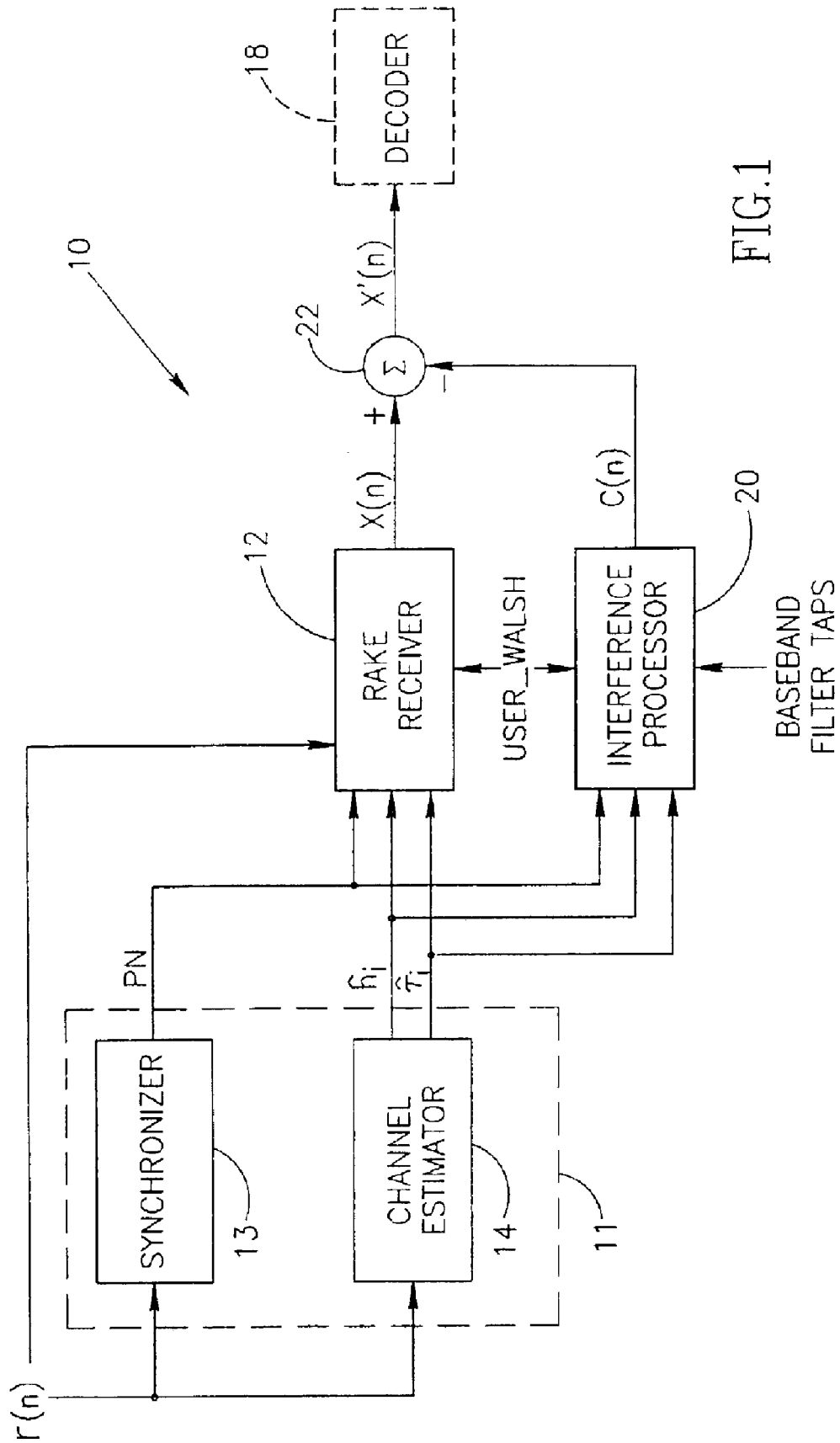


FIG. 1

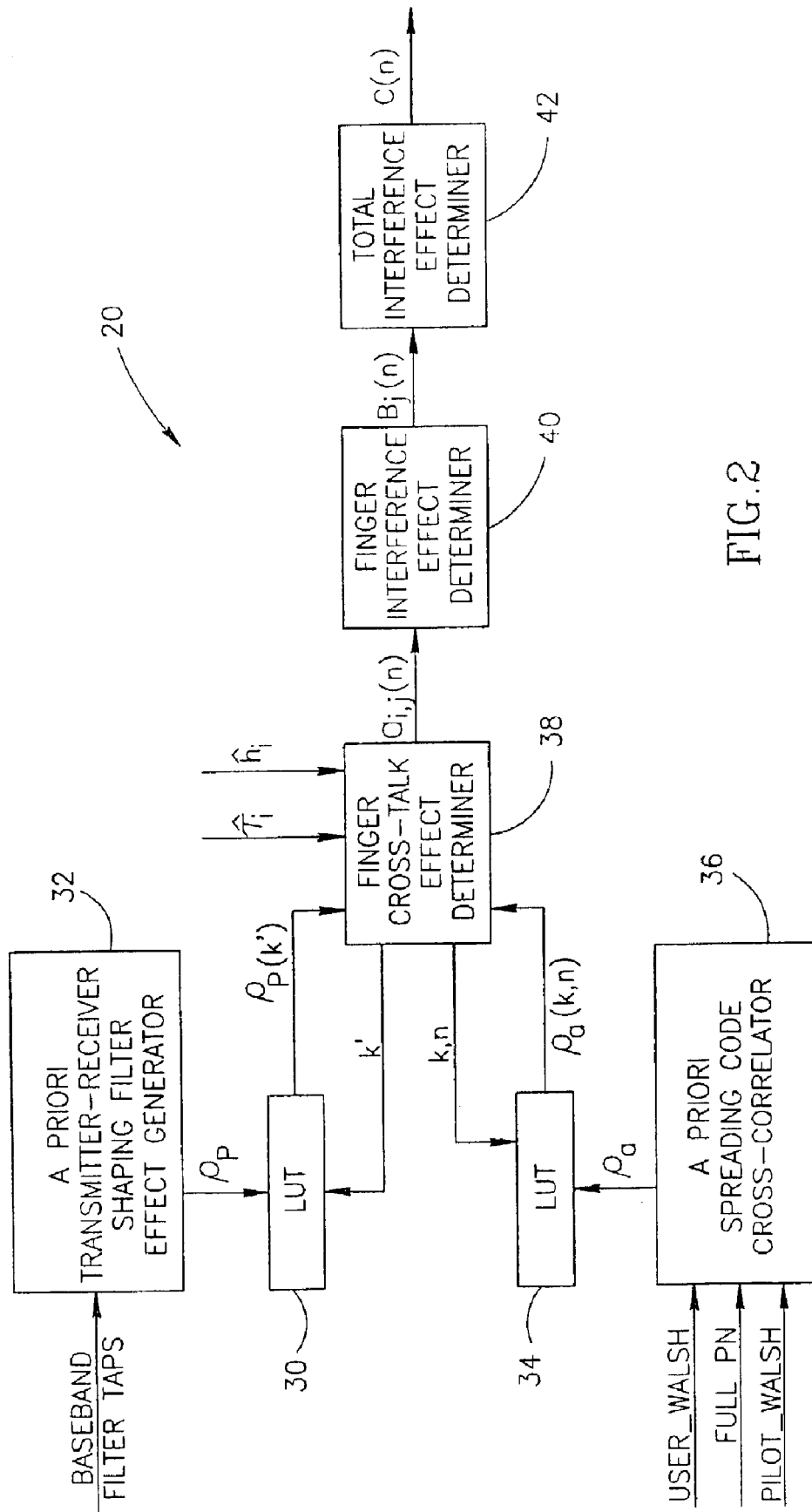


FIG. 2

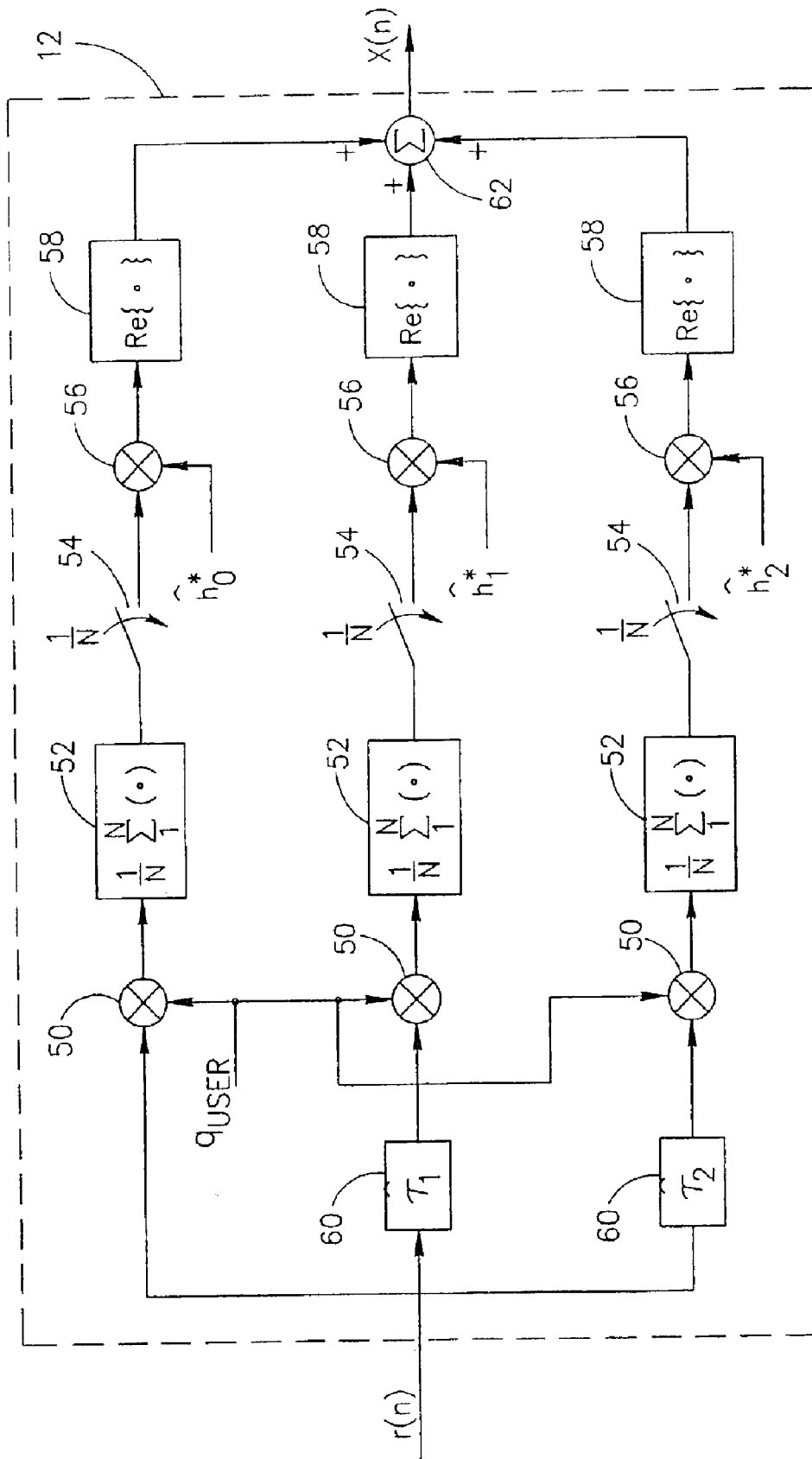


FIG. 3A
PRIOR ART

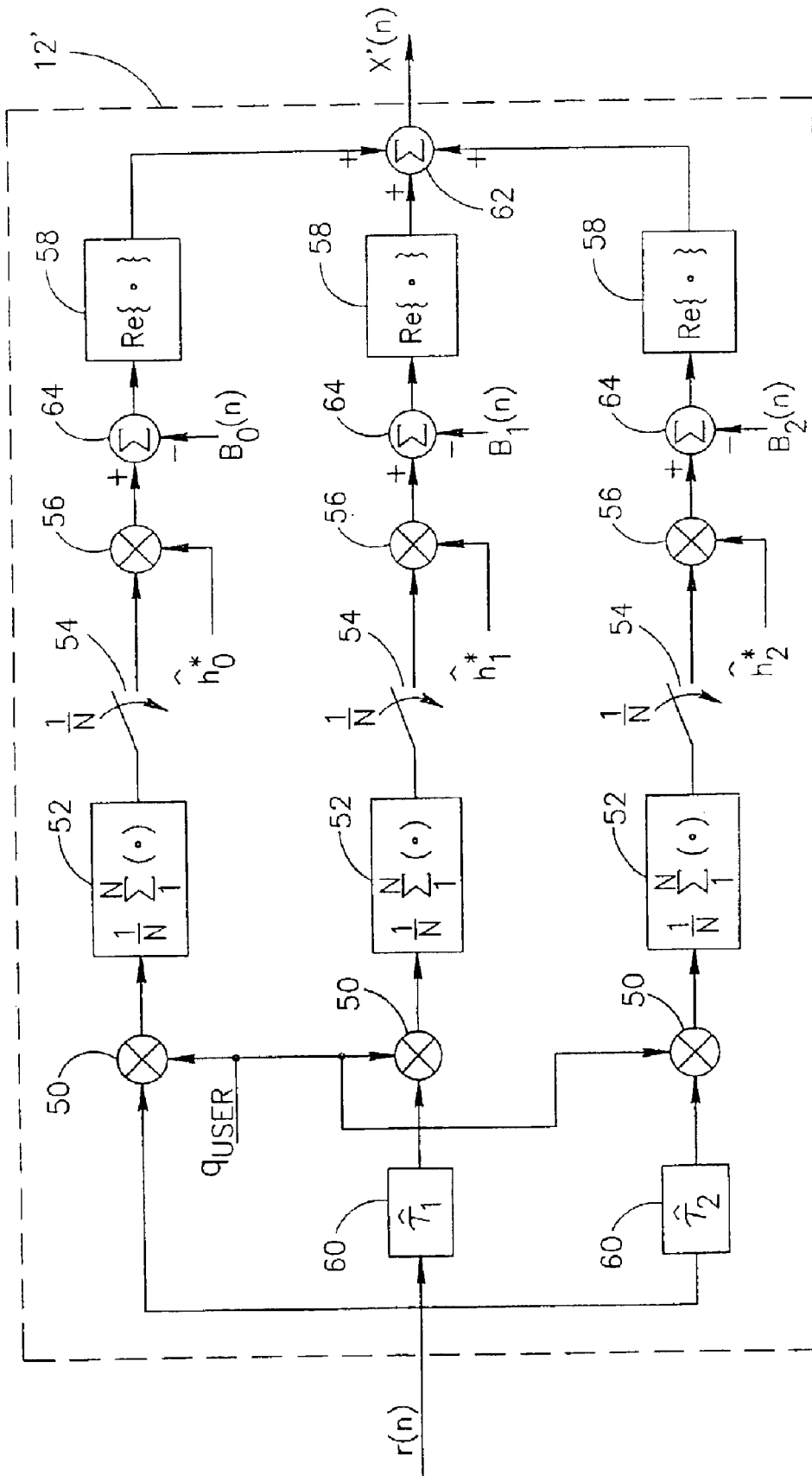


FIG. 3B

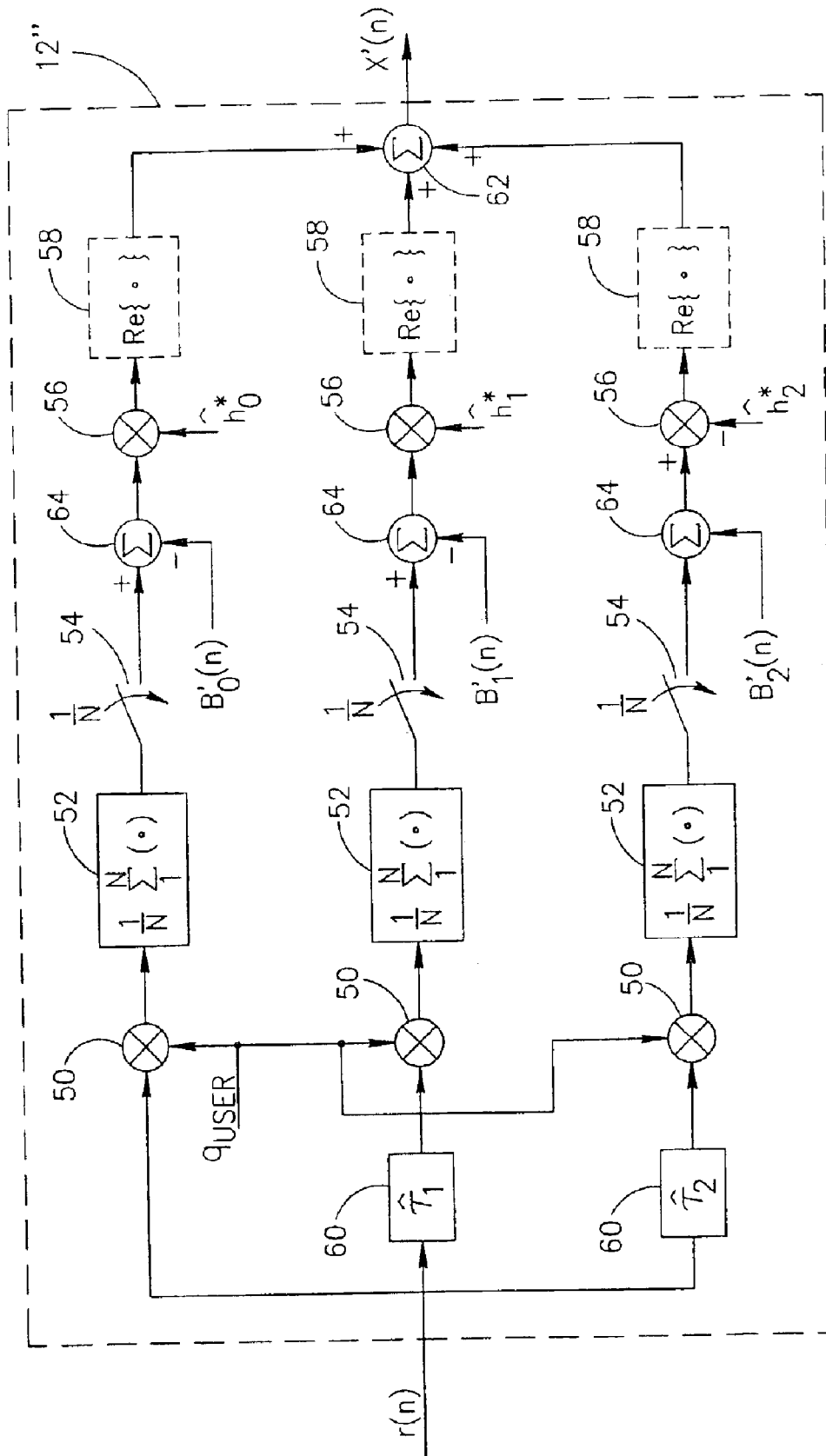


FIG. 3C

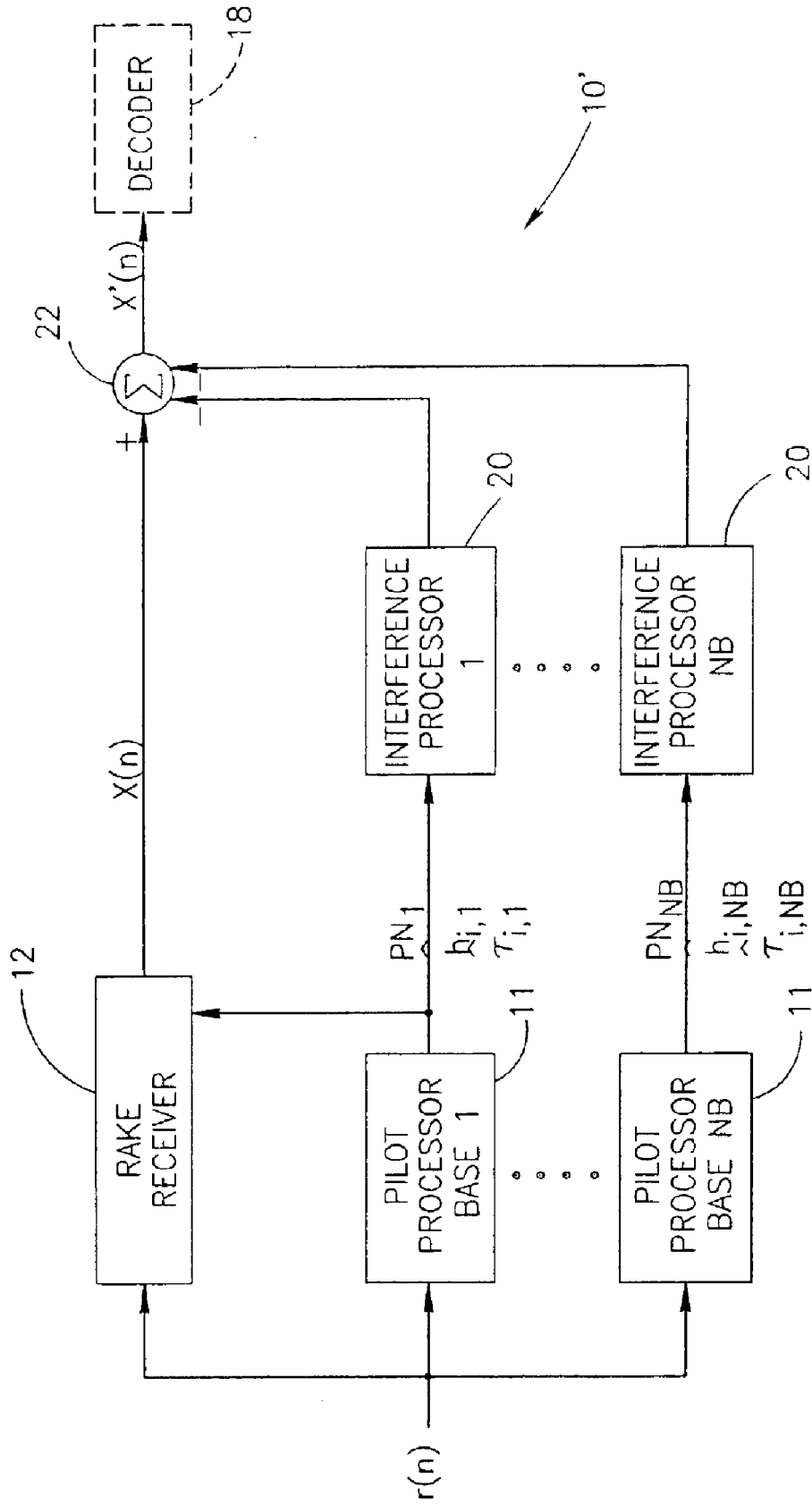


FIG. 4

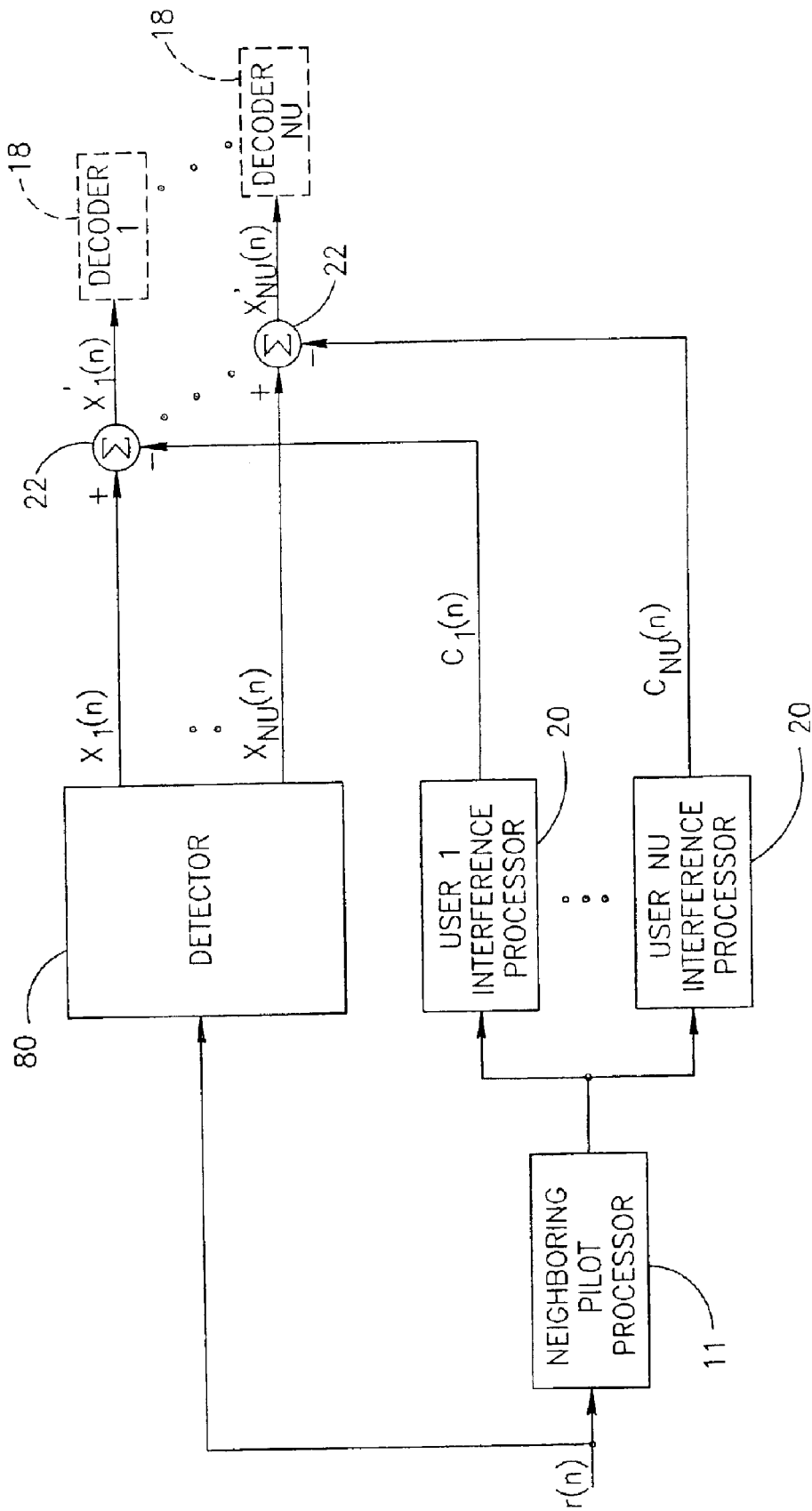


FIG. 5

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METHOD AND APPARATUS FOR REDUCING SPREAD SPECTRUM NOISE

CROSS-REFERENCE TO PREVIOUS APPLICATIONS

The present application is a continuation of U.S. Ser. No. 09/983,775 filed Oct. 25, 2001 (pending), which is a continuation-in-part of U.S. Ser. No. 09/443,864 filed Nov. 19, 1999, now U.S. Pat. No. 6,628,701 which is a continuation of U.S. Ser. No. 08/873,880 filed Jun. 11, 1997 (U.S. Pat. No. 6,034,986).

FIELD OF THE INVENTION

The present invention relates to spread spectrum communication systems generally and to noise reducing units in mobile handsets of such communication systems in particular.

BACKGROUND OF THE INVENTION

A conventional spread spectrum signal can be viewed as the result of mixing a narrowband information-bearing signal $i[t]$ with an informationless wideband "spreading" signal $p[t]$. If B_i and B_p denote the bandwidths of $i[t]$ and $p[t]$, respectively, then the "processing gain" available to the receiver is $G=B_p/B_i$. The receiver synchronizes the incoming signal to a locally generated version $p_o[t]$ of $p[t]$ and mixes the received signal with $p_o[t]$, thereby removing $p[t]$ from the signal and "collapsing" the signal to the "information bandwidth" B_i .

The spreading signal $p[t]$ is typically a coding sequence of some kind, such as a pseudo-random code. The United States space program initially utilized a Type 1 Reed-Muller code for deep-space communications. In many code division multiple access (CDMA) systems, the code is an M-sequence which has good "noise like" properties yet is very simple to construct.

For example, in the IS-95 standard for cellular communication, the forward channel (base to mobile units) employs, as a spreading code, the product of a 64 chip Walsh code (aimed at separating up to 64 different users per base) and a periodic PN sequence (aimed at separating the different bases). Thus, the spreading signal $p[t]$ for each user is its Walsh code combined with the current 64 chips of the PN sequence of its base station.

In order to synchronize the local version $p_o[t]$ of the spreading signal with the original version $p[t]$, the base station additionally transmits the current PN sequence via a pilot signal $z[t]$ (the pilot signal $z[t]$ is simply the current PN sequence multiplied by the all 1 Walsh code). The mobile unit then synchronizes its local code generator to the pilot signal after which the mobile unit can despread the received information bearing signals using its Walsh code and the current PN sequence.

The Walsh codes $W_i, i=1, \dots, 64$ are perfectly orthogonal to each other such that, in a non-dispersive transmission channel, there will be complete separation among the users even despite being transmitted at the same time and on the same transmission frequencies.

Practical channels, however, are time dispersive, resulting in multipath effects where the receiver picks up many echoes of the transmitted signal each having different and randomly varying delays and amplitudes. In such a scenario, the code's orthogonality is destroyed and the users are no longer separated. Consequently, a mobile unit, when attempting to detect only a single user, regards all other channel users

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(including signals from other base stations) as creators of interference. This contributes to a decrease in signal-to-noise ratio (SNR) and thus, reduces the reception quality of the mobile unit.

5 In the presence of multipath channels, the mobile units additionally process the informationless pilot signal to identify and track the multipath parameters of the channel. For this purpose, the mobile units include a channel estimator which detects and tracks the attenuation, denoted by channel "tap" \hat{h}_i , and the relative delay, denoted by $\hat{\tau}_i$, for each of the main paths. The mobile units then utilize the channel information in their detection operations.

One exemplary multipath detector is a rake receiver which optimally combines the different paths into a single replica of the transmitted signal. Rake receivers are described in detail e.g. in the book *Digital Communications* by J. G. Proakis, McGraw-Hill, Third Edition, 1995. The book is incorporated herein by reference.

A multiple-user detection scheme, such as is often used in base stations, can be viewed as interpreting the cross-talk between the signals of the users as merely a part of the multiple-input, multiple-output channel distortion. The base station accounts for this distortion during the detection process and, in general, the distortion does not translate into an SNR reduction. Therefore, it is not surprising that, with practical multipath channels, multi-user detection schemes are far superior to single-user ones.

BRIEF DESCRIPTION OF THE DRAWINGS

The present invention will be understood and appreciated more fully from the following detailed description taken in conjunction with the drawings in which:

FIG. 1 is a block diagram illustration of a data detector for a mobile unit, constructed and operative in accordance with an embodiment of the present invention;

FIG. 2 is a block diagram illustration of an interference processor useful in the detector of FIG. 1;

FIG. 3A is a block diagram of a standard receiver useful in the data decoder of FIG. 1;

FIGS. 3B and 3C are block diagrams of a pilot interference removing rake receiver, constructed and operative in accordance with alternative embodiments of the present invention;

FIG. 4 is a block diagram illustration of an alternative data detector for a mobile unit which removes the interference effect of multiple pilot signals, constructed and operative in accordance with an embodiment of the present invention; and

FIG. 5 is a block diagram illustration of a base station multi-user data detector constructed and operative in accordance with an embodiment of the present invention.

DETAILED DESCRIPTION OF PREFERRED EMBODIMENTS

Reference is now made to FIGS. 1 and 2 which illustrate a first embodiment of the mobile unit data detector of the present invention. FIG. 1 illustrates the detector in general and FIG. 2 illustrates the elements of an interference processor forming part of the detector of FIG. 1.

Detector 10 forms part of a mobile communication unit which receives a signal $r(n)$ and comprises a rake receiver 12, a pilot processor 11 and an optional decoder 18. The pilot processor 11 includes a synchronizer 13 and a channel estimator 14. However, in accordance with an embodiment

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of the present invention, detector **10** also comprises an interference processor **20** which utilizes the output of the existing channel estimator **14** and synchronizer **13**.

The signal $r(n)$ is the version of the received signal after the latter has been filtered and down converted to a baseband signal and has been sampled at rate of M samples per chip and N chips per symbol where M and N are typically integers. In the IS-95 CDMA standard, there are 64 chips per symbol n and the chip rate is 1.2288×10^6 chips per second, i.e. T_{chip} is about $0.8 \mu\text{sec}$. For simplicity, M is set to 1, i.e. upon receipt, the signal $r(n)$ is sampled once per chip.

Synchronizer **13** synchronizes the detector to the PN sequence of the base station and provides the current PN sequence to the rake receiver **12** and the interference processor **20**. Channel estimator **14** estimates the channel tap \hat{h}_i and the delay $\hat{\tau}_i$ associated with each finger. Rake receiver **12** despreads the user data signal of the current user using the user's Walsh code (which is known a priori), the current PN sequence, the estimated channel taps \hat{h}_i and the estimated finger delays $\hat{\tau}_i$. Rake receiver **12**, shown in detail in FIG. **3A**, produces the estimated user data signal $x(n)$, sampled once per symbol.

It is noted that the received signal $r(n)$ consists of the data signals of all of the active users (of the current base station and possibly of other, neighboring base stations) the pilot signals of at least the current base station and other interference terms caused by different noise sources in transmission, reception, etc. For the present discussion, the "pilot signal" will refer to the pilot signal of the current base station which is, by far, the strongest pilot signal received by the mobile unit.

In accordance with an embodiment of the present invention, interference processor **20** determines the cross-talk interference effect $c(n)$ of the pilot signal on the user data signal $x(n)$. Since the power of the pilot signal is typically significantly larger than that of any other channel user (to ensure that every synchronizer **13** can synchronize to it), removing the interference effect $c(n)$ of the pilot signal (via a subtractor **22**) should considerably improve the estimated user data signal $x(n)$. Furthermore, as described hereinbelow, the interference effect is relatively simple to calculate and thus, interference processor **20** can generally easily be implemented in a mobile handset where the computational burden must be minimized.

Subtractor **22** removes the interference effect $c(n)$ from the rake receiver output $x(n)$ thereby producing a new version $x'(n)$ of the data signal. The new version $x'(n)$ is decoded, via known methods, by optional decoder **18**.

Interference processor **20** determines the cross-talk through the rake receiver **12** due to the pilot signal and from this, generates the interference effect caused by the pilot signal. The cross-talk is of the form $\text{Re}\{\hat{h}_i \hat{h}_j^* \rho_a(k,n) \rho_p(k')\}$, $i \neq j$, where $*$ indicates the complex conjugate, the function $\text{Re}\{\}$ indicates the real portion of a complex number, $\rho_a(k,n)$ is the cross-correlation of the user and pilot spreading codes for the n th transmitted symbol, $\rho_p(k')$ depends on the baseband filter taps and defines the effect of transmit and receive shaping filters on a transmitted signal, k is a delay defined in integral chips (i.e. k is an integer number) and k' is a delay defined in fractional chips (i.e. k' is a real number). Typically, k' is measured in units of T_{chip}/M .

Since the baseband filter taps are known a priori and do not change over time, $\rho_p(k')$ can be determined a priori for all possible values of k' and stored in a lookup table **30**. A

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priori transmitter-receiver shaping filter effect generator **32** determines $\rho_p(k')$ as follows:

$$\rho_p(k') = \int_{-\infty}^{\infty} \alpha(t-k')\beta(-t)dt \quad \text{Equation 1}$$

where k' typically varies from $-L^{T_{chip}}/M < k' < L^{T_{chip}}/M$ in steps of T_{chip}/M , $\alpha(t)$ is the impulse response of the overall transmit shaping filter and $\beta(t)$ is the impulse response of the overall receive shaping filter. Since $\rho_p(k')$ decays as k' increases, L is chosen to indicate that point where $\rho_p(k')$ is very small. In other words, L is chosen such that $\rho_p(L^{T_{chip}}/M) < \rho_p(0)$. The transmit filter impulse response $\alpha(t)$ is defined in the IS-95 and IS-98 CDMA standards. For IS-95 it is found in section 6.1.3.1.10 "Baseband Filtering" (pages 6-31-6-33 of IS-95-A+TSB74). The receive filter impulse response $\beta(t)$ is a design option and is typically chosen to be equal to $\alpha(t)$ in order to maximize the expected signal to noise ratio. The impulse responses $\alpha(t)$ and $\beta(t)$ are thus known a priori. The output of generator **32** is stored in lookup table **30**, per value of k' .

Since all Walsh codes and the entire PN sequence are known a priori (recall that the PN sequence is finite and periodic), and since each symbol is transmitted with N values of the PN sequence, $\rho_a(k,n)$ can also be generated a priori, for all possible values of k and n and stored in a lookup table **34**. A priori spreading code cross-correlator **36** determines $\rho_a(k,n)$ as follows.

$$\rho_a(k, n) = \frac{1}{2N} \sum_{m=0}^{N-1} q_{pilot}(m+k, s) q_{user}(m, n)^* \quad \text{Equation 2}$$

$$q_x(m, n) = x_{Walsh}(m) * PN(m+nN)$$

$$x = \text{pilot or user}$$

$$0 \leq m \leq L-1 \text{ per symbol } n$$

$$-\infty \leq n \leq \infty$$

$$PN(m+nN+kQ) = PN(m+nN) \forall m, n, k$$

where, as defined in the above equation, the pilot and user Walsh codes $q(m,n)$ are sequences of N chips and $PN(n)$ is a periodic extension of a pseudo-random number sequence of length Q where, for the IS-95 standard, Q is 2^{15} .

Interference processor **20** additionally comprises a finger cross-talk determiner **38** which receives the estimated channel taps \hat{h}_i and the estimated finger delays $\hat{\tau}_i$ from the channel estimator **14** and utilizes them and the information stored in the two lookup tables **30** and **34** to determine the cross-talk effect of two fingers i,j for the given channel, channel delays and pilot signal.

Specifically, interference processor **20** begins by determining the value of k_0' , where $k_0' = \hat{\tau}_i - \hat{\tau}_j$, after which interference processor **20** activates cross-talk effect determiner **38** to determine the cross-talk effect $a_{i,j}(n)$ as follows:

$$a_{i,j}(n) = \sum_{k,k'} \text{Re}\{\hat{h}_i \hat{h}_j^* \rho_a(k, n) \rho_p(k')\} \quad \text{Equation 3}$$

where the sum is performed for all k and k' within the ranges around k_0' defined by $|k - \text{int}(k_0')| < J$ and $|k' - k_0'| < J$, respectively. J is a design parameter and is typically in the range of 1 to 10. It is noted that the delay differences k' and k are stepped by steps of one chip, where all delay difference k' includes the fractional portion of k_0' . Thus, if k_0' is, for

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example, 7.25 chips, then k' might have values of 5.25, 6.25, 7.25, 8.25 and 9.25 and k might have values 5, 6, 7, 8 and 9.

Equation 3 is operative for BPSK signaling. For non-BPSK signaling, such as QPSK signaling, Equation 3 becomes:

$$a_{i,j}(n) = \sum_{k,k'} \hat{h}_i \hat{h}_j^* \rho_a(k, n) \rho_p(k') \quad \text{Equation 4'}$$

The quantity $a_{i,j}(n)$ can be shown to be an estimate of the interference of the pilot signal along finger i to the user signal at finger j . Any number of fingers can be assumed though three is common. For three fingers, i and j vary from 0 to 2. In the IS-95 standard the Walsh codes are perfectly orthogonal, the term $a_{i,j}(n)$ is identically zero. However, with non-orthogonal codes, this term is generally non-zero.

To calculate $a_{i,j}(n)$, interference processor 20 retrieves the value of $\rho_a(k, n)$ for each value of k and for the n th symbol from lookup table 34 and the value of $\rho_p(k')$ for each value of k' from lookup table 30. Interference processor 20 activates the cross-talk effect determiner 38 for each set (i, j) of fingers where, for each set, the value of k_0' is first determined as are the ranges of k and k' .

Interference processor 20 additionally comprises a finger interference effect determiner 40 and a total interference effect determiner 42. Finger interference effect determiner 40 determines the interference effect $B_j(n)$ per finger as:

$$B_j(n) = \sum_i a_{i,j}(n) \quad \text{Equation 5}$$

where the sum is performed over the number of fingers in the channel.

Total interference effect determiner 42 determines the total interference effect $C(n)$ as the sum of the $B_j(n)$. The total interference effect $C(n)$ is the output of interference processor 20. As shown in FIG. 3B described in detail hereinbelow, the rake receiver 12 can subtract the individual finger interferences $B_j(n)$ from the individual finger contribution, thereby directly producing the corrected, estimated user data signal $x'(n)$.

It will be appreciated that, by removing the interference effect of the pilot signal, a significant portion, though not all, of the noise which affects the user signal $x(n)$ has been removed, thus increasing the performance quality of optional decoder 18. Furthermore, as can be seen from the discussion hereinabove, the computational burden of interference processor 20 is relatively small, in particular since the two cross-correlations $\rho_a(k, n)$ and $\rho_p(k')$ can be determined a priori and stored in the lookup tables 30 and 34. Alternatively, $\rho_a(k, n)$ can be determined "on-the-fly", from equation 2, since its computation only involves summation on PN "chips" which, in the IS-95 standard, accept only the values of ± 1 .

Reference is now briefly made to FIG. 3A which illustrates the elements of rake receiver 12 for a three finger channel and to FIGS. 3B and 3C which illustrate alternative versions 12' and 12'' of rake receiver 12 which performs the interference correction therewithin.

Rake receiver 12 has three fingers, each performing approximately the same operation on its associated finger. Each finger includes a despreader 50, a windowing summer 52, a sampler 54, a finger gain multiplier 56 and a complex-to-real converter 58. In addition, the second and third fingers include delays 60.

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The first finger, known as the 0th finger, serves as the reference finger. The second and third fingers (referred to as the 1st and 2nd fingers), respectively, have delays defined by τ_1 and τ_2 , respectively, relative to the 0th finger. Delays 60 delay the received signal $r(n)$ by their delay relative to the 0th finger. For completion, we set $\tau_0=0$.

Despreaders 50 despread the received signal $r(n)$ (the 0th finger) or the delayed signal (the 1st and 2nd fingers) via the spreading signal q_{user} defined hereinabove. Windowing summer 52 sums the output of despreaders 50 over a window of N samples and divides the result by N , as indicated. Samplers 54 sample every N th datapoint. Finger gain multipliers 56 multiply the sampled signal by the complex conjugate of the associated channel tap \hat{h}_j . Converters 58 take the real portion of the resultant signal. A summer 62 sums the output of each finger and produces therefrom the data signal $x(n)$.

The rake receiver 12' of FIG. 3B is similar to that of FIG. 3A (and therefore, similar elements carry similar reference numerals) with the addition of three subtractors 64 between their respective multiplier 56 and converter 58. Subtractors 64 subtract the finger interference effect $B_j(n)$ of the relevant finger from the output of the relevant multiplier 56.

It will be appreciated that, in this embodiment, the output of rake receiver 12' is the corrected data signal $x'(n)$.

The rake receiver 12'' of FIG. 3C is similar to that of FIG. 3B except that the interference effect is subtracted from the output of despreaders 50. For this, the three subtractors 64 are found before (rather than after) their respective multiplier 56. Furthermore, converter 58 is optional. The cross-talk effect $a_{i,j}(n)$ for this embodiment is now:

$$a'_{i,j}(n) = \sum_{k,k'} \text{Re}\{\hat{h}_i \rho_a(k, n) \rho_p(k')\} \quad \text{Equation 5}$$

for BPSK signaling and

$$a'_{i,j}(n) = \sum_{k,k'} \hat{h}_i \rho_a(k, n) \rho_p(k') \quad \text{Equation 5'}$$

for non-BPSK signaling.

$$B'_j(n) = \sum_i a'_{i,j}(n) \quad \text{Equation 6}$$

Reference is now briefly made to FIG. 4 which illustrates a data detector 10' capable of reducing multi-pilot interference. The detector of FIG. 4 is particularly useful for mobile units when they are approximately equidistant between two or more base stations. At this position, the mobile units receive the pilot signals of the multiple base stations with approximately equal strength. Both pilot signals interfere with the transmitted data signal.

The data detector 10' is similar to data detector 10 of FIG. 1 in that it includes rake receiver 12, subtractor 22 and optional decoder 18. Data detector 10' also includes a plurality NB of interference processors 20, one per base station that is interfering, and associated pilot processors 11. As described hereinabove, each pilot processor 11 includes a synchronizer, a channel estimator and a delay estimator. However, in data detector 10', each pilot processor 11 synchronizes to the pilot of a different base station and, accordingly, each interference processor 20 generates the interference effect of the pilots of the different base stations. Subtractor 22 removes the multiple interference effect out-

puts of processors 20 from the data signal x(n) in order to produce the corrected signal x'(n) which optional decoder 18 then decodes.

It will be appreciated that the pilot and interference processors 11 and 20, respectively may also be incorporated in a base station. In this embodiment, the processors 11 and 20 operate on the NU user signals which the base station receives. Thus, as shown in FIG. 5, the base station includes a detector 80 which produces NU data signals x_i(n). In accordance with an embodiment of the present invention, the base station includes at least one pilot processor 11 for the neighboring base station's pilot signal and NU interference processors 20, one per user, for determining the interference effect of the neighboring pilot signal on the data signal of each user. The base station also includes NU subtractors 22, one per user, for removing the interference effect C_i(n) of the relevant interference processor 20 from the corresponding data signal x_i(n).

It will be appreciated by persons skilled in the art that the present invention is not limited to what has been particularly shown and described hereinabove. Rather the scope of the present invention is defined only by the claims which follow.

The invention claimed is:

1. A method, comprising:

detecting a received signal that includes a pilot signal; and subtracting an interference signal from a data signal, the interference signal being a result of the pilot signal; and said subtracting including subtracting a combined cross-talk interference and a finger interference from the data signal.

2. A method as claimed in claim 1, wherein said subtracting includes subtracting a cross-talked interference effect of the pilot signal on the data signal.

3. A method as claimed in claim 1, wherein said subtracting includes subtracting an individual finger interference from an individual finger contribution of the data signal.

4. A method as claimed in claim 1, further comprising decoding a version of the data signal that represents the data signal with the combined cross-talk interference and the finger interference subtracted therefrom.

5. An apparatus, comprising:

a detector circuit to detect a received signal that includes a pilot signal; and

a subtractor circuit to subtract an interference signal from a data signal contained in the received signal, the interference signal being a result of the pilot signal and including a combined cross-talk interference and a finger interference.

6. An apparatus as claimed in claim 5, said subtractor circuit to subtract a cross-talk interference effect of the pilot signal on the data signal.

7. An apparatus as claimed in claim 5, said subtractor circuit to subtract an individual finger interference from an individual finger contribution of the data signal.

8. An apparatus as claimed in claim 5, further comprising a decoder circuit to decode a version of the data signal that represents the data signal with the combined cross-talk interference and the finger interference subtracted therefrom.

9. An apparatus, comprising:

means for detecting a received signal that includes a pilot signal; and

means, for subtracting an interference signal from a data signal contained in the received signal, the interference signal being a result of the pilot signal and including a combined cross-talk interference and a finger interference.

10. An apparatus as claimed in claim 9, said means for subtracting to subtract a cross-talk interference effect of the pilot signal on the data signal.

11. An apparatus as claimed in claim 9, said means for subtracting to subtract an individual finger from an individual finger contribution of the data signal.

12. An apparatus as claimed in claim 9, further comprising means for decoding a version of the data signal that represents the data signal with the combined cross-talk interference and the finger interference subtracted therefrom.

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